

On Fairness Optimization for NOMA-Enabled Multi-Beam Satellite Systems

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Abstract—In a multi-beam satellite communication system, traffic requests are typically asymmetric across beams and highly heterogeneous among terminals. In practical operations, it is important to achieve a good match between the offered and requested traffic, i.e., to improve the performance of Offered Capacity to requested Traffic Ratio (OCTR). Due to satellites’ payload constraints and limited flexibilities, it is a challenging task for resource optimization. In this paper, we tackle this issue by formulating a max-min resource allocation problem, taking fairness into account such that the lowest OCTR can be maximized. To exploit the potential synergies, we introduce Non-Orthogonal Multiple Access (NOMA) to enable aggressive frequency reuse and mitigate intra-beam interference. Although NOMA has proven its capabilities in improving throughput and fairness in 5G terrestrial networks, for multi-beam satellite systems it is unclear if NOMA can help to enhance the OCTR performance, and hence is worth quantifying how much gain it can bring. To solve the problem, we design a suboptimal algorithm to firstly decompose the original problem into multiple convex subproblems by fixing power allocation for each beam, and secondly adjust beam power to improve the minimum OCTR in iterations. Numerical results show the convergence of the proposed algorithm and the superiority of the proposed NOMA scheme in max-min OCTR.

I. INTRODUCTION

From Cisco’s prediction, the amount of wireless and mobile traffic will occupy 71% of total traffic by 2022, and the traffic distribution will be heavily imbalanced over a wide range of geographical areas [1]. The upward trend and traffic asymmetry necessitate the development of new types of data-service techniques. With the advantages of wide coverage, service continuity, and fiber-like data transmission, using satellites to serve terrestrial terminals, e.g., satellite-based backhauling [2], is envisioned as one of the most promising transmission solutions. A multi-beam satellite system is suited to provide reliable and low-cost wireless services to rural areas which incumbent terrestrial mobile systems are hard to reach.

In practical satellite operations, one of the issues is the presence of mismatches between the requested traffic and the offered capacity [3]. This is because, firstly, in a multi-beam satellite system, the requested traffic from terrestrial terminals are highly asymmetric. Secondly, the satellite resource allocation in multi-beam systems is constrained by satellites’ payload design, e.g., limited flexibility in

bandwidth, time, or power allocation. As a consequence, it could happen that, in some spot beams, the requested demands from the associated terminals are unmet, resulting in hot beams, whereas the offered capacity in some other beams is unused, leading to cold beams. Both of them are undesirable cases for satellite operators because the former loses revenue corresponding to the unmet demands, and the latter wastes the investment in the unused capacity [3]. Therefore, the capability to overcome this issue by allocating on-board resources over the service coverage is becoming a must for future broadband multi-beam satellites. To well capture the impact of unmet and excess capacity, resource optimization for the Offered Capacity to requested Traffic Ratio (OCTR) has been considered in the literature [3].

As an emerging research area, some efforts have been devoted to introducing 5G new radio techniques, e.g., Non-Orthogonal Multiple Access (NOMA), to satellite scenarios, in order to further enhance the satellite performance. The major consideration is that, with breaking the orthogonality, multiple terminals in NOMA can access the same time-frequency resource simultaneously, which improves the spectrum efficiency compared to Orthogonal Multiple Access (OMA) in DVB-S2 standards [4]. In addition, performing Multi-User Detection (MUD) and Successive Interference Cancellation (SIC) in NOMA can help to alleviate co-channel interference [5]. Thus NOMA has potentials to enable aggressive frequency reuse but suppress interference at an acceptable level in satellite systems. In [6], NOMA was considered for satellite scenarios for the first time. Two user-scheduling algorithms were proposed in their work to maximize the capacity for over-loaded satellite systems. From a system-level point of view, the authors in [7] analyzed the possibility and applicability of integrating NOMA to satellite systems and provided general approaches for cooperating NOMA with precoding. In [8], the authors considered a satellite-terrestrial system and applied NOMA in the terrestrial part. A joint user pairing, precoding, and power allocation scheme was proposed.

From the literature, NOMA has proven its advantages, e.g., throughput, energy [5], [9], over OMA in terrestrial

systems. However, for satellite systems, the optimization for the practical metric OCTR is studied to a limited extent, motivating us to fathom this area. The contribution of the paper lies at the following aspects:

- This paper aims at providing answers and algorithmic solutions for the following two research questions: Firstly, is NOMA able to improve the OCTR performance in satellite systems? Secondly, how much is the gain of applying NOMA to the considered problem?
- We consider a max-min resource optimization problem in NOMA-based multi-beam satellite systems, taking OCTR metric and terminals' fairness into account. The problem aims at improving the performance of the terminal with the worst OCTR such that the optimized capacity for terminals can be as close as their requested traffic demands and the fairness among terminals can be improved.
- To solve the problem, firstly we decompose the original problem into multiple convex subproblems by fixing beam power and find the optimum for each beam. Secondly, we iteratively adjust beam power to progressively improve the minimum OCTR.

Numerical results show the convergence of the proposed algorithm. The algorithm also demonstrates the superiority of NOMA over the OMA scheme.

II. SYSTEM MODEL

A. Multi-Beam Satellite Systems

We consider the forward link transmission in a multi-beam satellite system, where a Geostationary Earth Orbit (GEO) satellite is equipped with an array-fed reflector antenna with multiple feeds to generate B spot beams (one feed per beam) and provide services to number of K_b ground terminals per beam. Let $b = 1, \dots, B$ and \mathcal{B} be the index and set of beams, respectively, where $|\mathcal{B}| = B$. We denote $k = 1, \dots, K_b$ and \mathcal{K}_b as the index and set of the associated terminals in beam b , respectively, where $|\mathcal{K}_b| = K_b$. Let $\mathbf{h}_{bk} \in \mathbb{C}^{1 \times B}$ be the channel vector of terminal k in beam b . The m -th element of \mathbf{h}_{bk} , i.e., $h_{bk}^{(m)}$, indicates the channel coefficient from the m -th beam feed to terminal k in beam b , which can be expressed as $h_{bk}^{(m)} = L_{mbk} G_{bk}^r G_{mbk}^s$, where L_{bk} is the free-space propagation loss from the m -th feed to the k -th terminal. G_{bk}^r is the k -th terminal's receive antenna gain. G_{mbk}^s is the gain from the m -th feed to the k -th terminal in beam b . By adopting NOMA, we let all the beams share the same frequency band, i.e., 1-color reuse pattern. In terms of payload, we assume that the on-board payload is equipped with the module of flexible Multi-Port Amplifiers (MPAs) such that power can be adjusted.

B. Precoding and NOMA Scheme

Let $\mathbf{w}_b \in \mathbb{C}^{B \times 1}$ denote the precoding vector for beam b . For terminal k in beam b , the received signal can be

expressed as:

$$y_{bk} = \underbrace{\mathbf{h}_{bk} \mathbf{w}_b \sqrt{p_{bk}} s_{bk}}_{\text{desired signal}} + \underbrace{\mathbf{h}_{bk} \mathbf{w}_b \sum_{j \neq k} \sqrt{p_{bj}} s_{bj}}_{\text{intra-beam interference}} + \underbrace{\mathbf{h}_{bk} \sum_{b' \neq b} \mathbf{w}_{b'} \sum_{l \in \mathcal{K}_{b'}} \sqrt{p_{b'l}} s_{b'l}}_{\text{inter-beam interference}} + n_{bk}, \quad (1)$$

where p_{bk} , s_{bk} , and $n_{bk} \sim \mathcal{CN}(0, \sigma^2)$ are the transmit power, the transmit signal with unit power, and the additive noise for terminal k in beam b , respectively.

In the paper, we use precoding to reduce inter-beam interference, while NOMA is adopted to eliminate part of intra-beam interference for multiple terminals within a beam. We adopt a linear precoding scheme, Minimum Mean Square Error (MMSE), which is considered with high efficiency and low computational complexity [6], [10]. For MMSE, we denote $\mathbf{H} \in \mathbb{C}^{B \times B}$ as the channel matrix. The b -th row represents the channel vector of the terminal with the maximum channel coefficient in beam b [8], i.e., $\arg \max_{k \in \mathcal{K}_b} \{|h_{bk}^{(b)}|^2\}$, where $h_{bk}^{(b)}$ is the channel coefficient of terminal k in beam b when receiving its desired signal from the b -th feed. The precoding matrix reads:

$$\mathbf{W}_{mmse} = (\mathbf{H}^H \mathbf{H} + \sigma^2 \mathbf{I})^{-1} \mathbf{H}^H, \quad (2)$$

where \mathbf{I} is the identity matrix. In this paper, we do not discuss precoding design but power allocation for beams and terminals. The power of each precoding vector is then normalized as $\|\mathbf{w}_b\|^2 = 1$.

Within a beam, NOMA is applied to mitigate intra-beam interference among the terminals. According to a widely adopted approach for determining decoding order [11], we define the SIC decoding order as the descending order of the ratio between channel gain to inter-beam interference plus noise, denoted by g_{bk} :

$$g_{bk} = \frac{|\mathbf{h}_{bk} \mathbf{w}_b|^2}{\sum_{b' \neq b} |\mathbf{h}_{bk} \mathbf{w}_{b'}|^2 P_{b'} + \sigma^2}, \quad (3)$$

where $P_{b'} = \sum_{l \in \mathcal{K}_{b'}} p_{b'l}$. We note that in this paper g_{bk} refers to the channel condition of each terminal. We use vector \mathbf{P} to collect all the beam power $P_1, \dots, P_b, \dots, P_B$. The rationale is that, if terminal j can decode the signal of terminal k , in order to ensure a successful SIC, the SINR of terminal k 's signal at terminal j 's receiver should be higher than that at terminal k , then (3) is used to guarantee this inequality [11].

Based on the NOMA basis [11], a terminal k , before decoding its own signal, first performs SIC to decode and subtract the signals from the terminals whose channel conditions are worse than k , whereas the signals from the terminals with better channel conditions than k are treated as noise. We define that $\phi_b(k)$ is the position of decoding orders in beam b . If $\phi_b(k) < \phi_b(j)$, then $g_{bk} > g_{bj}$

and terminal k can decode the signals of terminal j . The decoding order position of the terminal with the best channel condition is $\phi_b(k) = 1$, whose SINR γ_{bk} can be expressed as,

$$\gamma_{bk} = \frac{|\mathbf{h}_{bk}\mathbf{w}_b|^2 p_{bk}}{\sum_{b' \neq b} |\mathbf{h}_{bk}\mathbf{w}_{b'}|^2 P_{b'} + \sigma^2}. \quad (4)$$

This terminal has the highest ratio g_{b1} , and is able to remove all the intra-beam interference. For any terminals with $\phi(k) > 1$, the SINR γ_{bk} is,

$$\gamma_{bk} = \frac{|\mathbf{h}_{bk}\mathbf{w}_b|^2 p_{bk}}{\sum_{\phi(k') < \phi(k)} |\mathbf{h}_{bk}\mathbf{w}_b|^2 p_{bk'} + \sum_{b' \neq b} |\mathbf{h}_{bk}\mathbf{w}_{b'}|^2 P_{b'} + \sigma^2}. \quad (5)$$

The achievable rate of terminal k in beam b is

$$R_{bk} = \log(1 + \gamma_{bk}). \quad (6)$$

III. PROBLEM FORMULATION

In this section, we formulate a power allocation problem in $\mathcal{P}1$ to max-min OCTR among terminals, in which the optimization variables are p_{bk} , $\forall b \in \mathcal{B}$, $\forall k \in \mathcal{K}_b$.

$$\mathcal{P}1 : \max_{\{p_{bk}\}} \min_{b \in \mathcal{B}, k \in \mathcal{K}_b} \left\{ \frac{R_{bk}}{D_{bk}} \right\} \quad (7a)$$

$$\text{s.t.} \quad \sum_{b \in \mathcal{B}} \sum_{k \in \mathcal{K}_b} p_{bk} \leq P_{tot}, \quad (7b)$$

$$\sum_{k \in \mathcal{K}_b} p_{bk} \leq P_{b,\max}, \forall b \in \mathcal{B}. \quad (7c)$$

In the objective, the OCTR metric for terminal k in beam b is defined as $\frac{R_{bk}}{D_{bk}}$, where R_{bk} and D_{bk} are the offered capacity and the requested traffic, respectively. By optimization, the terminals' fairness can be enhanced by improving the worst-OCTR terminal's performance. Constraint (7b) states that due to the limited on-board power supply, the total power should be less than a budget P_{tot} . In (7c), the allocated power to each feed should be constrained by a peak power $P_{b,\max}$, to avoid nonlinear impairments in on-board high-power amplifiers.

Remark 1. In $\mathcal{P}1$, the ideal case is $\frac{R_{bk}}{D_{bk}} = 1$ for all the terminals. We do not impose constraints as $\frac{R_{bk}}{D_{bk}} \leq 1$ or $\frac{R_{bk}}{D_{bk}} \geq 1$, such that the fluctuation of OCTR around one can be observed.

The problem can be equivalently transformed to $\mathcal{P}2$ by introducing an auxiliary variable t .

$$\mathcal{P}2 : \max_{\{p_{bk}\}, t} t \quad (8a)$$

$$\text{s.t.} \quad \sum_{b \in \mathcal{B}} \sum_{k \in \mathcal{K}_b} p_{bk} \leq P_{tot}, \quad (8b)$$

$$\sum_{k \in \mathcal{K}_b} p_{bk} \leq P_{b,\max}, \forall b \in \mathcal{B}, \quad (8c)$$

$$\frac{R_{bk}}{D_{bk}} \geq t, \forall b \in \mathcal{B}, k \in \mathcal{K}_b. \quad (8d)$$

Some approaches based on standard interference function, e.g., [13], and Perron-Frobenius theory, e.g., [14], were proposed to enable a convergence guaranteed solution to interference control problems. If the decoding order in each beam remains constant for any power allocation, the problem satisfies the specific conditions of these approaches and can be solved. However, in the most general scenarios, it is impractical to keep decoding orders always the same while adjusting transmit power. With the changes of decoding orders, the function R_{bk} is no longer continuous at the point where decoding orders change, which makes the original problem non-convex and much more difficult to solve. Even though the approaches based on standard interference function and Perron-Frobenius theory are mature, these approaches cannot be applied directly since the function R_{bk} is not continuous and does not satisfy the specific conditions of these approaches. Thus we need to decompose the original problem and propose a heuristic algorithm to solve the problem.

IV. PROPOSED ALGORITHMIC SOLUTION

To solve $\mathcal{P}2$, firstly we consider decomposing the optimization task into two levels, i.e., intra-beam and inter-beam. The former is to find the maximum t_b within each beam by fixing beam power. The latter aims at adjusting power P_1, \dots, P_B among beams to progressively improve the minimum value of t_b .

A. Power Optimization within Each Beam

Specifically, we divide $\mathcal{P}2$ into number of B subproblems with fixed beam power for the moment. In this phase, the decoding order within each beam is fixed. The subproblem for beam b can be formulated as:

$$\mathcal{P}3 : \max_{p_{b1}, \dots, p_{b|\mathcal{K}_b|}, t_b} t_b \quad (9a)$$

$$\text{s.t.} \quad \sum_{k \in \mathcal{K}_b} p_{bk} \leq P_b, \quad (9b)$$

$$\frac{R_{bk}}{D_{bk}} \geq t_b, \forall k \in \mathcal{K}_b, \quad (9c)$$

where P_b in (9b) represents the total allocated power for beam b . The value of P_b can be further tuned to meet the constraints (7b) and (7c) over iterations. Next, we show that, by fixing the beam power, the allocation problem $\mathcal{P}3$ is a convex problem. By adopting the substituting method in [5], we can express p_{bk} by a function of R_{bk} , e.g., $p_{b1} = \frac{e^{R_{b1}} - 1}{g_{b1}}$ and $p_{b2} = \frac{e^{R_{b2}} - 1}{g_{b2}} (g_{b2} \frac{e^{R_{b1}} - 1}{g_{b1}} + 1)$ for a two-terminal example. $\mathcal{P}3$ can be equivalently transformed to

$\mathcal{P}4$ by treating $R_{b1}, \dots, R_{b|\mathcal{K}_b|}$ as variables.

$$\mathcal{P}4 : \max_{R_{b1}, \dots, R_{b|\mathcal{K}_b|}, t_b} t_b \quad (10a)$$

$$\text{s.t.} \sum_{k \in \mathcal{K}_b} \left(\frac{1}{g_{b[\phi_b(k)]}} - \frac{1}{g_{b[\phi_b(k)-1]}} \right) e^{(\sum_{\phi_b(j) \geq \phi_b(k)} R_{bj})} - \frac{1}{g_{b[\Phi_b]}} \leq P_b, \quad (10b)$$

$$t_b D_{bk} - R_{bk} \leq 0, \forall k \in \mathcal{K}_b, \quad (10c)$$

where we denote $[\phi_b(k)]$ as the index of the terminal whose decoding order position is $\phi_b(k)$. Φ_b denotes the decoding order position of the terminal with the worst channel condition and $[\Phi_b]$ denotes the index of this terminal. Constraint (10b) with the form of sum exponential functions therefore concludes the convexity of (10b) as well as $\mathcal{P}4$ [12].

B. Power Optimization Among Beams

Deriving Karush-Kuhn-Tucker (KKT) conditions for $\mathcal{P}4$, the optimal value of t_b can be obtained by the following equation,

$$\sum_{k \in \mathcal{K}_b} \left(\frac{1}{g_{b[\phi_b(k)]}} - \frac{1}{g_{b[\phi_b(k)-1]}} \right) e^{(\sum_{\phi_b(j) \geq \phi_b(k)} R_{bj})} - \frac{1}{g_{b[\Phi_b]}} - P_b = 0, \quad (11)$$

where $t_b D_{bj} = R_{bj}$ at the optimum. However, the closed-form expression of t_b by power P_1, \dots, P_B is hard to derive. From (11), we then express t_b in an implicit way, i.e., $t_b(\mathbf{P}) = t_b(P_1, \dots, P_B)$. Thus, to obtain the max-min OCTR, the task can be carried out by optimizing P_1, \dots, P_B instead of tuning power for each terminal. The corresponding optimization problem $\mathcal{P}5$ reads,

$$\mathcal{P}5 : \max_{P_1, \dots, P_B} \min_{b \in \mathcal{B}} \{t_b(P_1, \dots, P_B)\} \quad (12a)$$

$$\text{s.t.} \sum_{b \in \mathcal{B}} P_b \leq P_{tot}, \quad (12b)$$

$$P_b \leq P_{b, \max}, \forall b \in \mathcal{B}. \quad (12c)$$

We remark that $\mathcal{P}5$ may not be with an appropriate formulation to derive a complete solution due to lack of the explicit expression in the objective. However, deriving a necessary condition for the optimum of $\mathcal{P}5$ is possible by applying the rule of implicit differentiation. The result is elaborated in **Lemma 1**.

Lemma 1. *Suppose η is the optimal objective value of $\mathcal{P}5$, then $t_b(P_1, \dots, P_B) = \eta, \forall b \in \mathcal{B}$.*

Proof. Suppose η is optimal to $\mathcal{P}5$ and $t_b = \eta$ for beam b while $t_{b'} > \eta$ for $\forall b' \neq b \in \mathcal{B}$. Even though it is hard to obtain the closed-form expression of $t_b(P_1, \dots, P_B)$, we can analytically derive the partial derivatives as $\frac{\partial t_b(\mathbf{P})}{\partial P_b} = \frac{1}{G(\mathbf{P})}$ and $\frac{\partial t_b(\mathbf{P})}{\partial P_{b'}} = \frac{F(\mathbf{P})}{G(\mathbf{P})}$, where

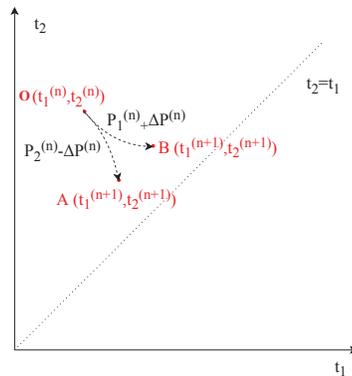


Fig. 1. Illustration of the proposed algorithm.

$$G(\mathbf{P}) = \sum_{k \in \mathcal{K}_b} \left(\frac{1}{g_{b[\phi_b(k)]}} - \frac{1}{g_{b[\phi_b(k)-1]}} \right) \cdot e^{\sum_{\phi_b(j) \geq \phi_b(k)} t D_{bj}} \sum_{\phi_b(j) \geq \phi_b(k)} D_{bj}, \quad (13)$$

$$F(\mathbf{P}) = \sum_{k \in \mathcal{K}_b} (\beta_{b[\phi_b(k)]b'} - \beta_{b[\phi_b(k)-1]b'}) \cdot e^{\sum_{\phi_b(j) \geq \phi_b(k)} t D_{bj}} - \beta_{b[\Phi_b]b'}, \quad (14)$$

and $\beta_{b[\phi_b(k)]b'} = \frac{|\mathbf{h}_{b[\phi_b(k)]} \mathbf{w}_{b'}|^2}{|\mathbf{h}_{b[\phi_b(k)]} \mathbf{w}_b|^2}$. Since $\frac{\partial t_b(\mathbf{P})}{\partial P_b} > 0$ but $\frac{\partial t_b(\mathbf{P})}{\partial P_{b'}} < 0$, we can reduce power of any beam b' or/and increase power of beam b to raise t_b . Thus there exists $\eta' > \eta$ with a feasible solution, which contradicts the assumption. \square

C. The Proposed Algorithm

The aim of the algorithm is to improve the minimal value of t_b . Since it is hard to identify the properties of $\mathcal{P}5$, we propose an iterative methodology to find a suboptimal solution. We will illustrate the methodology with the two-beam case.

From **Lemma 1** we know that the necessary condition of obtaining the optimal solution to $\mathcal{P}5$ is $t_1 = t_2$. Therefore we design the algorithm to increase the value of $\eta = \min_{b=1,2} \{t_b\}$ as much as possible until the condition $t_1 = t_2$ holds. At the n -th iteration of the algorithm, if $\eta^{(n)} = t_1^{(n)} < t_2^{(n)}$, for instance, there are two ways to enhance the value of η : $P_1^{(n)} + \Delta P^{(n)}$ or $P_2^{(n)} - \Delta P^{(n)}$. Suppose the step size $\Delta P^{(n)}$ is small enough. When $P_2^{(n)}$ decreases by the value of $\Delta P^{(n)}$, the variations of t_1 and t_2 can be approximately derived as: $t_1^{(n+1)} - t_1^{(n)} \approx -\frac{\partial t_1}{\partial P_2} \Delta P^{(n)}$, $t_2^{(n+1)} - t_2^{(n)} \approx -\frac{\partial t_2}{\partial P_2} \Delta P^{(n)}$. With the specific precoding method MMSE, $\beta_{b[\phi_b(k)]b'}$ is relatively small compared to 1. So we can derive approximately that $|\frac{\partial t_1}{\partial P_2}| < |\frac{\partial t_2}{\partial P_2}|$ according to the expressions of the partial derivatives of t_b . Then $|t_1^{(n+1)} - t_1^{(n)}| < |t_2^{(n+1)} - t_2^{(n)}|$. Similarly, when $P_1^{(n)}$ increases by $\Delta P^{(n)}$, $|t_1^{(n+1)} - t_1^{(n)}| > |t_2^{(n+1)} - t_2^{(n)}|$. This indicates that enhancing P_1 can head to the path gaining

Algorithm 1 The proposed algorithm

- 1: Initialize $\mathbf{P}^{(0)}$ satisfying constraints in $\mathcal{P}5$.
 - 2: Set the maximal number of iterations N , $n = 0$, $\mathbf{t}^{(0)} = (t_1^{(0)}, \dots, t_B^{(0)}) = \mathbf{0}$.
 - 3: Solve (11) and obtain $\mathbf{t}^{(0)}$ with $\mathbf{P}^{(0)}$, $\eta = \min_{b \in \mathcal{B}} \{t_b^{(0)}\}$.
 - 4: **repeat**
 - 5: Select $\underline{b} \leftarrow \arg \min_{b \in \mathcal{B}} \{t_b^{(n)}\}$, $\bar{b} \leftarrow \arg \max_{b \in \mathcal{B}} \{t_b^{(n)}\}$.
 - 6: **if** $P_{\underline{b}}^{(n)} < \min \{P_{\underline{b}, \max}, P_{tot} - \sum_{b \neq \underline{b}} P_b^{(n)}\}$ **then**
 - 7: Update: $\Delta P \leftarrow \min \{P_{\underline{b}, \max}, P_{tot} - \sum_{b \neq \underline{b}} P_b^{(n)}\}$.
 - 8: **repeat**
 - 9: Calculate \mathbf{t}' and $\eta' \leftarrow \min_{b \in \mathcal{B}} \{t_b'\}$ with $P_{\underline{b}}^{(n)} + \Delta P$.
 - 10: Update: $\Delta P \leftarrow \Delta P/2$.
 - 11: **until** $\eta' > \eta$ or ΔP is small enough
 - 12: Update $\mathbf{P}^{(n+1)}$.
 - 13: **else**
 - 14: Update: $\Delta P \leftarrow P_{\underline{b}}/2$.
 - 15: **repeat**
 - 16: Calculate \mathbf{t}' and $\eta' \leftarrow \min_{b \in \mathcal{B}} \{t_b'\}$ with $P_{\bar{b}}^{(n)} - \Delta P$.
 - 17: Update: $\Delta P \leftarrow \Delta P/2$.
 - 18: **until** $\eta' > \eta$ or ΔP is small enough
 - 19: Update $\mathbf{P}^{(n+1)}$.
 - 20: Update: $\mathbf{t}^{(n+1)} \leftarrow \mathbf{t}'$, $\eta \leftarrow \eta'$, $n \leftarrow n + 1$.
 - 21: **until** $n = N$ or η converges
 - 22: Output: $\mathbf{P} \leftarrow \mathbf{P}^{(n)}$, $\mathbf{t} \leftarrow \mathbf{t}^{(n)}$
-

larger η than reducing P_2 . The variation tendencies of t_1 and t_2 while altering P_1 and P_2 are depicted in Fig. 1. Thus for the beam with smaller t_b , the effective way to improve t_b is to gain more transmit power rather than reduce power of other beams.

The algorithm is described in Alg. 1. At each iteration, it identifies if the power of the beam with the smallest t_b is smaller than the maximum limitation. If so, it chooses to improve this beam's power (line 7-12). In this phase, the step size ΔP is first initialized as the gap between its power level and the maximal power limitation. If η gets larger after power rises, ΔP will be determined; otherwise, ΔP is halved. If the power of the beam with the smallest t_b reaches the maximum limitation, it is designed to reduce power of the beam with the largest t_b (line 14-19), in order to enhance the minimal value of t_b . In this phase, ΔP can be set as half of its power. ΔP will be upgraded the same as the process of the first phase.

V. PERFORMANCE EVALUATION

In this section, we evaluate the performance of the considered NOMA scheme and the proposed algorithm. The key parameters are summarized in TABLE I. In NOMA, since the MUD receivers' complexity increases

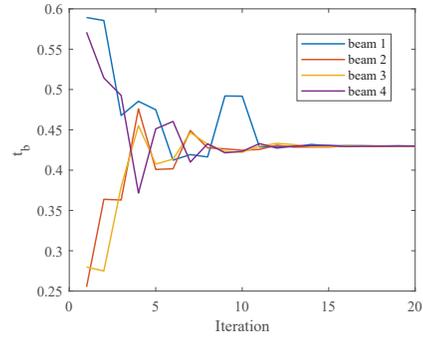


Fig. 2. Evolution of t_b in 4 beams over iterations in Algorithm 1

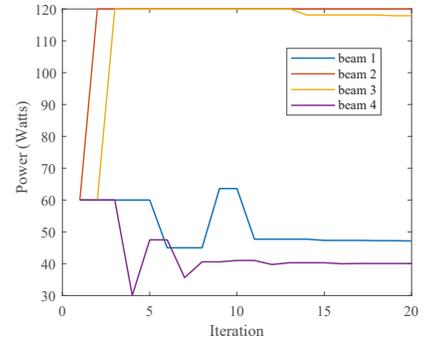


Fig. 3. Evolution of P_b in 4 beams over iterations in Algorithm 1

exponentially with the number of signals to be detected [7], in this work we limit the number of terminals per beam to two. In total, we deploy 70 terminals in each beam. At each run of the simulation, we select two of them in each beam. One terminal is chosen randomly first and the other one with large difference of channel gain is then paired [6]. The results are averaged over 1000 instances. The terminals' demands are uniformly distributed between 1 and 5 bits/s/Hz. To evaluate the performance of the proposed scheme, we adopt OMA with precoding and 1-color reuse pattern, NOMA with 2-color reuse pattern (without precoding), NOMA with 4-color reuse pattern (without precoding), OMA with 1-color reuse pattern (without precoding), and NOMA with 1-color reuse pattern (without precoding) for comparison.

Firstly, in Fig. 2 and 3, we evaluate the proposed Algorithm 1 for the NOMA with precoding and 1-color

TABLE I
SIMULATION PARAMETERS

Parameter	Value
Frequency	20 GHz (Ka band)
Bandwidth	500 MHz
Satellite location	13° E
Satellite height	35,786 km
Satellite antenna gain	between 49.60 and 54.63 dBi
Receive antenna gain	42.1 dBi
Channel	LoS channel (path loss)
Noise power (σ^2)	-126.47 dBW
Number of beams (B)	4
$P_{b, \max}, P_{tot}$	120, 400 W [14]

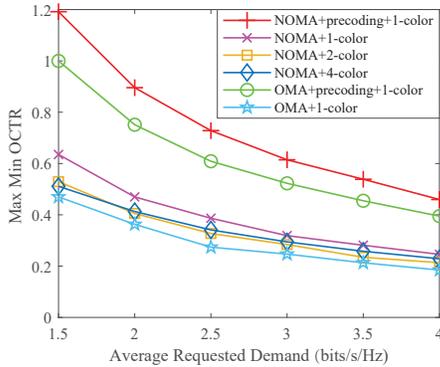


Fig. 4. Max-min OCTR in Algorithm 1 with respect to traffic demand.

reuse pattern. We show the Algorithm 1's evolution over iterations in terms of OCTR value t_b and beam power P_b , respectively. From the two Figures, we can observe that if a beam with lower value of t_b in an iteration, e.g., see the curves of beam 2 and 3 in iteration 1 in Fig. 2 and 3, at the next iteration, the algorithm will assign more power to compensate t_2 and t_3 , whereas the beams 1 and 4 in iteration 1 with the higher OCTR will be assigned by less power in later iterations. From Fig. 2, the algorithm demonstrates promising performance in convergence. Around 11 iterations, the max-min OCTR value approaches to the convergence point though with the long-tail effect. Analogous to Fig. 2, the power allocation for each beam converges around 13 iterations in Fig. 3.

Next, we use Fig. 4 to show the max-min OCTR performance among six schemes. From the results, the scheme of NOMA with precoding and 1-color reuse pattern outperforms. This is because the scheme is largely benefited from efficient frequency utilization and inter/intra-beam interference mitigation. In addition, when applying NOMA with 1-color reuse pattern, the performance is better than NOMA with 4-color as well as 2-color. The reason can be explained below. In 2-color and 4-color schemes, less inter-beam interference presents. To improve the max-min OCTR performance, one way is to increase the transmit power in a beam, say beam b . When the transmit power has achieved the peak power limitation $P_{b,max}$, the other way is then adopted to reduce the inter-beam interference by decreasing power $P_1, \dots, P_{b-1}, P_{b+1}, \dots, P_B$. As a result, when transmit power meets the limitation $P_{b,max}$, the max-min OCTR performance in 1-color scheme can be further improved by reducing the power in the other beams, whereas the 2/4-color reuse pattern gains less improvement due to less inter-beam interference, thus it results in performance gaps among 1-color, 2-color, and 4-color schemes.

VI. CONCLUSION

In this paper, we consider a NOMA-based multi-beam satellite system, and address a fairness issue in resource optimization. We aim at maximizing the worst OCTR performance by power optimization, such that the offered

and requested traffic can achieve a good match among terminals. The formulated max-min OCTR problem is non-convex in general scenarios. To solve the problem, we decompose the power optimization into each beam, and propose a suboptimal algorithm to enhance the fairness among terminals by sequentially and iteratively optimizing beam power. The simulation results show the convergence of the proposed algorithm, and the performance gain of NOMA than other baseline schemes. The numerical results demonstrate that NOMA is able to enhance the max-min OCTR performance, and the performance could be further improved when more aggressive frequency reuse schemes, e.g., 1-color, are adopted.

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